SPECIFICATION

TITLE OF THE INVENTION

SPREAD-SPECTRUM SIGNAL RECEIVER

BACKGROUND OF THE INVENTION

5   This invention relates to a spread-spectrum signal receiver for receiving a signal (referred to as a spread-spectrum signal) that has been spread by a direct-sequence (DS) scheme. More particularly, the invention relates to a spread-spectrum signal receiver

10   for receiving a spread-spectrum signal obtained by rendering transmit data and control data, which have been modulated at different powers, into signals that do not influence each other, e.g., signals that are mutually orthogonal, multiplexing these signals and

15   transmitting the multiplexed signal from a transmit side.

In spread-spectrum communications, W-CDMA (Wideband Code Division Multiple Access), which employs direct-sequence spreading, is one of the third-generation

20   mobile communications systems the standardization of which is being forwarded by the 3GPP (3rd Generation Partnership Project).

With CDMA, as shown in Fig. 9, a mobile station, which is a spread-spectrum signal transceiver, has a

25   first modulator 1a for applying BPSK modulation (see Fig. 10) to control data that includes pilot data, and a first spreader 1b for applying spread-spectrum modulation using a spreading code for the control data.

The mobile station further includes an encoding circuit 1c for subjecting the transmit data to suitable encoding such as convolutional coding a second modulator 1d for subsequently applying BSPK modulation and a second

5 spreader 1e for spreading the resultant signal using a spreading code for the transmit data. The mobile station further includes a multiplexer 1f for mapping the control data and transmit data, which have been spreaded by the first and second spreaders, as an I-axis

10 component (I-channel component) and Q-axis component (Q-channel component) of an I-Q complex plane, as illustrated on the right side of Fig. 10, and multiplexing the resulting signals, and a radio transmitter unit 1g for subjecting the multiplexed

15 signal to frequency conversion and high-frequency amplification and transmitting the resulting signal from an antenna 1h. It should be noted that the I and Q channels are referred to also as data and control channels, respectively.

20 An uplink signal from the mobile station to a base station has a frame format shown in Fig. 11. One frame has a duration of 10 ms and is composed of 15 slots S_0 to S_{14}. Transmit data is mapped to the I channel (data channel) and control data, which is data other than the

25 transmit data, is mapped to the Q channel (control channel). Each of the slots S_0 to S_{14} of the data channel that transmits the transmit data is composed of n bits, where n varies depending upon symbol rate. The

symbol rate will be 7.5 (= $5 \times 15/10 \times 10^{-3}$) kbps if n = 5 holds; 15 (= $10 \times 15/10 \times 10^{-3}$) kbps if n = 10 holds; 30 kbps if n = 20 holds, and so forth.

5   Each slot of the control channel that transmits the control data is composed of 10 bits, and the symbol rate is a constant 15 kbps. Each slot transmits a pilot, transmission-power control data TPC, a transport format combination indicator TFCI and feedback information FBI. The pilot is utilized on the receive side for coherent

10   detection and SIR (Signal to Interference Ratio) measurement, the TPC is utilized for control of transmission power, the TFCI transmits the symbol rate of the data and the number of bits per frame, etc., and the FBI is for controlling transmission diversity at the

15   base station.

Thus, there are instances where the symbol rates on the data and control channels differ. In such case the spreading factor [= (symbol rate)/(chip rate)] on the data channel differs from that on the control channel.

20   For example, (1) if the symbol rate of the data channel is lower than that (15 kbps) of the control channel, then the spreading factor of the data channel will be larger than that of the control channel, and (2) if the symbol rate of the data channel is higher than that (15

25   kbps) of the control channel, then the spreading factor of the data channel will be smaller than that of the control channel. The larger the spreading factor, the higher the process gain. Accordingly, in a W-CDMA

system, transmission power for which the spreading
factor is larger is reduced to lower the total
transmission power. In other words, with W-CDMA, the
control and data channels are subjected to BPSK and
5   spread-spectrum modulation at powers that differ from
each other, the spread-spectrum modulated signals are
mapped on an I-Q complex plane and multiplexed and the
multiplexed signal is transmitted.

If, by way of example, the spreading factor of the
10   data channel is larger than that of the control channel,
then, as shown in Fig. 12, the apparatus of Fig. 9 is
further provided with multipliers 1h, 1i, the multiplier
1h multiplies the BPSK modulation output of the second
modulator 1d of the data channel by β (β<1) and the
15   multiplier 1i multiplies the BPSK modulation output of
the first modulator 1a of the control channel by 1
(i.e., leaves this output unchanged). The first and
second spreaders 1b, 1e thenceforth spread-spectrum
modulate the outputs of the multipliers 1i, 1h,
20   respectively, the multiplexer 1f maps the spread-
spectrum modulated signals of the respective channels on
the I-Q complex plane, as illustrated in Fig. 13A, and
multiplexes the resultant signals, and the radio
transmitter unit 1g subjects the multiplexed signal to a
25   frequency conversion and high-frequency amplification
and transmits the resulting signal from the antenna 1h.
By thus lowering the transmission power of the channel
having the larger spreading factor, the total

transmission power can be controlled (reduced).

Further, if the spreading factor of the data channel is made smaller than that of the control channel, the multiplier 1h multiplies the BPSK

5   modulation output of the second modulator 1d by 1 and the multiplier 1i multiplies the BPSK modulation output of the first modulator 1a by β ($\beta<1$). The multiplexer 1f maps the spread-spectrum modulated signals of the respective channels on the I-Q complex plane, as

10   illustrated in Fig. 13B, and multiplexes the resulting signals. As a result, the total transmission power can be reduced by lowering the transmission power of the channel having the larger spreading factor.

Fig. 14 is a block diagram illustrating one channel

15   of the receiver section of a base station, which is a spread-spectrum signal transceiver. The base station has a radio unit 2a for frequency-converting a high-frequency signal received from an antenna ATN to a baseband signal; a quadrature demodulator 2b for

20   subjecting the baseband signal to quadrature detection, converting the analog in-phase component (I component) and analog quadrature component (Q component) to digital data and inputting the data to a searcher 2c and fingers $2d_1 \sim 2d_n$. Upon receiving input of a direct-sequence

25   signal (DS signal) that has been influenced by the multipath effect, the searcher 2C detects multipath interference by performing an autocorrelation operation using a matched filter and inputs despreading-start

timing data and delay-time adjustment data of each path to the fingers $2d_1 \sim 2d_n$. A control-channel despreader 3a of each of the fingers $2d_1 \sim 2d_n$ subjects a direct wave or delayed wave that arrives via a prescribed path

5   to despread processing using a code identical with the spreading code for the control channel, integrates the results of despreading, then applies delay processing that conforms to the path and outputs a control-data signal. A data-channel despreader 3b subjects a direct

10 wave or delayed wave that arrives via a prescribed path to despread processing using a code identical with the spreading code for the data channel, integrates the results of despreading, then applies delay processing that conforms to the path and outputs a transmit-data

15 signal.

A channel estimation unit 3c estimates the phasing characteristic of the propagation path using the pilot signal contained in the despread control-data signal, executes channel estimation which compensates for the

20 effects of phasing, and outputs a channel estimation signal. Channel compensation units 3d, 3e multiply the despread control-data signal and despread transmit-data signal by the complex-conjugate signal of the channel estimation signal to thereby compensate for phasing. A

25 RAKE combiner 2e combines the control-data signals output from the fingers $2d_1 \sim 2d_n$ and outputs the result as a soft-decision data sequence. A decision unit 2f renders the soft-decision data into hard decision data,

and a decoder 2g applies error-correction decoding

processing to the hard-decision data, which is output

from the decision unit 2f, decodes the control data that

prevailed prior to encoding and outputs the decoded

5 data. It should be noted that the soft-decision data,

rather than being made hard-decision data by the

decision unit 2f, can be subjected to soft-decision

error-correction processing by the decoder 2g as is,

whereby the control data is decoded and output. A

10 power-ratio calculation unit 2h calculates the ratio

$(Pd/Pc = \beta^2)$ of data-channel signal power Pd to control-

channel signal power Pc from the rate information

(symbol rate of the data) included in the TFCI bit of

the control data and outputs β.

15   A RAKE combiner 2i combines the control-data

signals output from the fingers $2d_1 \sim 2d_n$ and outputs the

result as a soft-decision data sequence. A delay add-on

unit 2j performs a time adjustment by delaying the soft-

decision data sequence long enough for the calculation

20 of the power ratio. A decision unit 2k multiplies the

soft-decision data level of the data channel by $1/\beta$ (the

level of the transmit-data signal is multiplied by β on

the transmit side) and then renders the data into hard

decision data. A decoder 2m applies error-correction

25 decoding processing to the hard-decision data, which is

output from the decision unit 2k, decodes the transmit

data that prevailed prior to encoding and outputs the

decoded data. It should be noted that the soft-decision

data that has been multiplied by $1/\beta$, rather than being made hard-decision data by the decision unit 2k, can be subjected to soft-decision error-correction processing by the decoder 2m as is, whereby the transmit data is

5   decoded and output.

Thus, in a case where a transmit-data signal and control-data signal are transmitted at different powers with the conventional spread-spectrum signal receiver, power-ratio information is computed based upon symbol-

10   rate information contained in the control data, the level of the transmit-data signal is changed based upon this information and then error-correction decoding processing is applied. With this method, however, a lengthy processing delay occurs by the time the power-

15   ratio information is acquired. For example, with W-DCMA, the symbol-rate information is transmitted over one frame (10 ms), as mentioned earlier, and therefore a minimum of 10 ms is required to acquire the power-ratio information. Further, the symbol-rate information is

20   encoded in order to improve its reliability, i.e., its reception characteristic, and therefore additional processing time is necessary to decode this information.

Information demanding delivery in real time, as in the case of voice communication, requires a short

25   communication delay, i.e., a short processing time. Further, a short processing time is desirable also in interference suppression techniques, such as in an interference canceller. Also required is a circuit such

as a memory for adding a processing delay onto the data
channel. The result is an increase in the scale of the
circuitry that is proportional to the amount of
processing delay.

5   SUMMARY OF THE INVENTION

Accordingly, an object of the present invention is
to shorten processing time for calculation of power
ratio.

Another object of the present invention is to make
10   it possible to decode transmit data and control data
correctly even in a case where the transmission powers
of the control data and transmit data are different.

A further object of the present invention is to
make it possible to correctly generate a replica used in
15   an interference canceller even in a case where the
transmission powers of the control data and transmit
data are different.

According to a first aspect of the present
invention, the foregoing objects are attained by
20   providing a spread-spectrum signal receiver for
receiving a signal obtained by rendering transmit data
and control data, which have been modulated at powers
that differ from each other, into signals (mutually
orthogonal signals) that do not influence each other,
25   multiplexing these signals and transmitting the
multiplexed signal from a transmit side, the apparatus
comprising: (1) a despreader for despreading a receive
signal to thereby demodulate a control-data signal and a

transmit-data signal; (2) a channel estimation unit for deriving a channel estimation value from a pilot signal that is contained in the control-data signal; (3) a channel compensation unit for performing channel

5   compensation of the transmit-data and control-data signals based upon the channel estimation value; (4) a power calculation unit for calculating power of the transmit-data signal and power of the control-data signal after the channel compensation and calculating a

10   power ratio representing the ratio of the calculated power of the transmit-data signal to the calculated power of the control-data signal; (5) a signal-level changing unit for raising, on the basis of the power ratio, the level of whichever of the signals has the

15   lower power; and (6) a decoder for executing decoding processing based upon the signal the level of which has been changed by the signal-level changing unit.

In accordance with the spread-spectrum signal receiver according to the first aspect of the invention,

20   the power ratio is not derived based upon symbol-rate information contained in control data as in the prior art. Rather, the power ratio is calculated upon obtaining the power of the transmit-data signal and the power of the control-data signal. This makes it

25   possible to shorten the processing time needed for calculating the power ratio. Further, the fact that processing time is shortened means that it is possible to reduce the scale of circuitry needed to add on a

processing delay.

Further, in accordance with the spread-spectrum signal receiver according to the first aspect of the invention, the level of whichever signal has been

5   reduced in power by having its signal level multiplied by β on the transmit side is multiplied by 1/β on the receive side, whereby the original level of the signal is restored. This is followed by the decoding of the signal. As a result, decoding can be performed

10   correctly even though the transmission powers of the control data and transmit data differ.

The signal-level changing unit in the spread-spectrum signal receiver of the first aspect of the present invention raises the level of the transmit-data

15   signal if the power ratio of transmit-data signal power to control-data signal power is less than 1 and raises the level of the control-data signal if the power ratio is greater than 1. As a result, even though the signal level of the transmit-data signal or of the control-data

20   signal is lowered on the transmit side, whichever signal level has been lowered can be restored automatically and decoding processing can be executed correctly on the receive side.

According to a second aspect of the present

25   invention, the foregoing objects are attained by providing a spread-spectrum signal receiver for receiving a signal obtained by rendering transmit data and control data, which have been modulated at powers

that differ from each other, into signals that do not influence each other, multiplexing these signals and transmitting the multiplexed signal from a transmit side, the apparatus comprising: (1) a despreader for despreading a receive signal to thereby demodulate a control-data signal and a transmit-data signal; (2) a channel estimation unit for deriving a channel estimation value from a pilot signal that is contained in the control-data signal; (3) a channel compensation unit for performing channel compensation of the transmit-data and control-data signals based upon the channel estimation value; (4) a power calculation unit for calculating power of the transmit-data signal and power of the control-data signal after the channel compensation and calculating a power ratio representing the ratio of the calculated power of the transmit-data signal to the calculated power of the control-data signal; (5) a decision unit for raising, on the basis of the power ratio, the level of whichever of the signals has the lower power, leaving unchanged the level of whichever of the signals has the higher power, and outputting control data and transmit data upon rendering a hard decision or soft decision based upon the signals of the changed level and the unchanged level; (6) means for changing replica reliability RC1 of the transmit data and replica reliability RC2 of the control data based upon the power ratio; and (7) a first replica generator for generating a replica of transmit data on

the transmit side by multiplying the transmit data, which is output from the decision unit, by the replica reliability RC1 conforming to the power ratio, and for generating a replica of control data on the transmit side by multiplying the control data, which is output from the decision unit, by the replica reliability RC2 conforming to the power ratio.

The spread-spectrum signal receiver according to the second aspect of the invention further comprises: means for changing replica reliability RC of the transmit signal based upon the power ratio; means for replicating the transmit signal by spreading the replicas of the transmit data and control data using spreading codes on the transmit side; and a second replica generator for generating a replica of the transmit signal by multiplying the replicated transmit signal by the replica reliability RC conforming to the power ratio.

Thus, the spread-spectrum signal receiver according to the second aspect of the present invention is so adapted that replica reliability is changed based upon the power ratio. More specifically, the higher the reception power, the higher the replica reliability is made. This makes it possible to raise the reliability of a generated replica. As a result, interference can be suppressed using each replica.

Other features and advantages of the present invention will be apparent from the following

description taken in conjunction with the accompanying drawings, in which like reference characters designate the same or similar parts throughout the figures thereof.

5 BRIEF DESCRIPTION OF THE DRAWINGS

Fig. 1 illustrates the flow of processing for power-ratio calculation from transmission to reception according to the present invention;

Fig. 2 is a block diagram of a CDMA receiver
10 according to a first embodiment;

Fig. 3 is a block diagram of a CDMA receiver according to a second embodiment;

Fig. 4 is a block diagram of a receiver having an interference canceller according to a third embodiment;

15 Fig. 5 is a block diagram of a symbol replica generator according to the third embodiment;

Fig. 6 illustrates an example of a conversion table according to the third embodiment;

Fig. 7 is a block diagram of an interference
20 replica generator according to a fourth embodiment;

Fig. 8 illustrates an example of a second conversion table according to the fourth embodiment;

Fig. 9 is a block diagram of a CDMA transmitter in a mobile station according to the prior art;

25 Fig. 10 is a diagram useful in describing BPSK modulation and mapping to an I-Q complex plane according to the prior art;

Fig. 11 illustrates the frame format of an uplink

frame according to the prior art;

Fig. 12 is a block diagram showing the transmitter section of a mobile station in W-CDMA according to the prior art;

5   Figs. 13A, 13B are diagrams useful in describing multiplexed signals in a complex plane according to the prior art; and

Fig. 14 is a block diagram illustrating one channel of a CDMA receiver section in the CDMA receiver of a

10   base station.

DESCRIPTION OF THE PREFERRED EMBODIMENTS

(A)   Flow of power-ratio calculation from
        transmission to reception

Fig. 1 illustrates the flow of processing for

15   power-ratio calculation from transmission to reception according to the present invention. It is assumed here that the symbol rate of the data channel is lower than that of the control channel, i.e., that the process gain of the data channel is higher.

20   A CDMA transmitter 11 serving as an example of a spread-spectrum signal receiver includes a multiplier 11a for multiplying BPSK-modulated control data $e^{j\theta}$ by a gain factor (= 1), and a spreader 11b for multiplying the output signal of the multiplier 11a by a spreading

25   code $e^{j\omega}$ to generate a spread-spectrum modulated signal $e^{j(\theta+\omega)}$ and sending this modulated signal to a propagation path 12. The CDMA transmitter 11 further includes a multiplier 11a' for multiplying BPSK-modulated transmit

data $e^{j\theta'}$ by a gain factor β (<1), and a spreader 11b'

for multiplying the output signal of the multiplier 11a'

by the spreading code $e^{j\omega}$ to generate a spread-spectrum

modulated signal $\beta e^{j(\theta'+\omega)}$ and sending this modulated

5   signal to the propagation path 12.

The spread-spectrum modulated signals $e^{j(\theta+\omega)}$, $\beta e^{j(\theta'+\omega)}$

that have been sent to the propagation path 12 undergo

phasing (amplitude fluctuation α and phase fluctuation

ϕ) and respectively become the signals

10    $\alpha e^{j(\theta+\omega+\phi)}$, $\alpha\beta e^{j(\theta'+\omega+\phi)}$

These signals are received by a CDMA receiver 13. In

Fig. 1, multipliers 12a, 12a' are provided for

multiplying the spread-spectrum modulated signals $e^{j(\theta+\omega)}$,

$\beta e^{j(\theta'+\omega)}$ by a phasing characteristic $\alpha e^{j\phi}$ to thereby

15   express the influence of phasing.

The CDMA receiver 13 includes a despreading

modulator 13a for performing despreading using a code

identical with the spreading code of the control data on

the transmit side, and outputting a despread signal

20   (control-data signal) $\alpha e^{j(\theta+\phi)}$, and a despreading

modulator 13a' for performing despreading using a code

identical with the spreading code of the transmit data

on the transmit side, and outputting a despread signal

(transmit-data signal) $\alpha\beta e^{j(\theta'+\phi)}$.

25   A multiplier 13b serving as a channel estimation

unit multiplies the control-data signal $\alpha e^{j(\theta+\phi)}$ output

from the despreading modulator 13a by an already known

pilot cancel signal $e^{-j\theta}$ to thereby calculate a channel

estimation value $\alpha e^{j\phi}$, and channel compensation units

13c, 13c' multiply the control-data signal $\alpha e^{j(\theta+\phi)}$ and

transmit-data signal $\alpha\beta e^{j(\theta'+\phi)}$, respectively, by the

complex-conjugate signal $\alpha e^{-j\phi}$ of the channel estimation

5　value to thereby perform phasing compensation and output

$\alpha^2 e^{j\theta}$, $\alpha^2\beta e^{j\theta'}$, respectively.

A power calculation unit 13d multiplies the

phasing-compensated control signal $\alpha^2 e^{j\theta}$ by its complex-

conjugate signal $\alpha^2 e^{-j\theta}$ and outputs power α^4 of the

10　control signal.　A power calculation unit 13d'

multiplies the phasing-compensated control signal $\alpha^2\beta e^{j\theta'}$

by its complex-conjugate signal $\alpha^2\beta e^{-j\theta'}$ and outputs power

$\alpha^4\beta^2$ of the data signal.　A power-ratio calculation unit

13e calculates the ratio β^2 between data-signal power Pd

15　and control-signal power Pc in accordance with the

following equation:

$$\beta^2 = Pd/Pc$$

and outputs β.

In summary, the CDMA transmitter 11 spread-spectrum

20　modulates control data and transmit data following the

BPSK modulation thereof, and the spread-spectrum

modulated signals sustain phasing in the propagation

path 12 and then enter the CDMA receiver 13.　The latter

compensates for phasing by performing channel

25　compensation processing using an estimation value

calculated from the pilot signal included in the

control-data signal and then calculates the power of the

control-data signal and the power of the transmit-data

signal and estimates the power ratio from these signal powers. The estimation of the power ratio does not require one frame of processing time, unlike the prior art. For example, if X symbols are used in order to

5   improve estimation precision at a symbol rate of 15 kbps (10 bits/slot, i.e., 150 bits/frame), the processing time needed to estimate the power ratio is X/15 (ms). Thus, the processing time needed to calculate the power ratio can be shortened greatly. Further, the scale of

10   circuitry needed to add on a delay can be reduced.

(B)   First embodiment

Fig. 2 is a block diagram illustrating one channel's worth of a CDMA receiver, which is a spread-spectrum signal transceiver according to the present

15   invention. Here it is assumed that the symbol rate of the transmit data is lower than that of the control data. That is, it is assumed that data is transmitted upon making β the gain factor of the transmit data and making 1 the gain factor of the control data.

20   The CDMA receiver includes a radio unit 21 for frequency-converting a high-frequency signal received from an antenna ATN to a baseband signal; a quadrature demodulator 22 for subjecting the baseband signal to quadrature detection, converting the analog in-phase

25   component (I component) and analog quadrature component (Q component) to digital data and inputting the data to a searcher 23 and fingers $24_1 \sim 24_n$. Upon receiving input of a direct-sequence signal (DS signal) that has

been influenced by the multipath effect, the searcher 23

detects multipath interference by performing an

autocorrelation operation using a matched filter and

inputs despreading-start timing data and delay-time

5   adjustment data of each path to the fingers $24_1 \sim 24_n$.

A control-channel despreader 24a of each of the

fingers $24_1 \sim 24_n$ subjects a direct wave or delayed wave

that arrives via a prescribed path to despread

processing using a code identical with the transmit-side

10   spreading code for the control channel and outputs a

control-data signal. A data-channel despreader 24b

subjects a direct wave or delayed wave that arrives via

a prescribed path to despread processing using a code

identical with the spreading code for the data channel

15   and outputs a transmit-data signal. A channel

estimation unit 24c performs channel estimation using

the pilot signal contained in the despread control-data

signal and outputs a channel estimation signal. Channel

compensation units 24d, 24e multiply the despread

20   control-data signal and despread transmit-data signal by

the complex-conjugate signal of the channel estimation

signal to thereby compensate for phasing.

A RAKE combiner 25 combines the control-data

signals output from the fingers $24_1 \sim 24_n$ and outputs the

25   result as a soft-decision data sequence. A RAKE

combiner 26 combines the transmit-data signals output

from the fingers $24_1 \sim 24_n$ and outputs the result as a

soft-decision data sequence. A power-ratio calculation

unit 27 (1) calculates the power Pc of the control-data
signal by multiplying the control-data signal output
from the RAKE combiner 25 by the complex-conjugate
signal of this control-data signal, (2) calculates the
5 power Pd of the transmit-data signal by multiplying the
transmit-data signal output from the RAKE combiner 26 by
the complex-conjugate signal of this transmit-data
signal, and (3) calculates the ratio β^2 (= Pd/Pc) between
these powers and outputs β.

10 Delay add-on units 28, 29 delay, by a length of
time needed for the calculation of the power ratio, the
soft-decision data sequence of the control data and the
soft-decision data sequence of the transmit data output
from the RAKE combiners 25, 26, respectively. A decoder
15 30 applies soft-decision error-correction decoding
processing to the soft-decision data sequence, which is
output from the delay add-on unit 28, decodes the
control data and outputs the decoded data.

A signal-level changing unit 31 multiplies the
20 level of the soft-decision data sequence output from the
delay add-on unit 29 by $1/\beta$, thereby restoring the level
of the transmit data that was multiplied by β on the
transmit side. A decoder 32 thenceforth applies soft-
decision error-correction decoding processing to the
25 soft-decision data sequence, which is output from the
signal-level changing unit 31, decodes the transmit data
and outputs the decoded data.

Though the soft-decision data sequences are input

to the decoders 30, 32 in the arrangement described above, hard-decision units can be provided in front of the decoders 30, 32 and hard-decision data sequences can be input to the decoders.

5   In accordance with the first embodiment, rather than the power ratio being calculated based upon symbol-rate information contained in control data, as in the prior art, the power ratio is calculated by finding the power of the transmit-data signal and the power of the control-data signal. This makes it possible to shorten

10   the processing time needed for calculation of the power ratio. Further, shortening the processing time makes it possible to reduce the scale of the circuitry constituting the delay add-on units 28, 29 which add on

15   the processing delay time. Further, in accordance with the first embodiment, the level of whichever signal has been reduced in power by having its signal level multiplied by β on the transmit side is multiplied by 1/β on the receive side, whereby the original level of

20   the signal is restored. This is followed by the decoding of the signal. As a result, decoding can be performed correctly even though the transmission powers of the control data and transmit data differ.

       (C)   Second embodiment

25   In the first embodiment, it is assumed that the symbol rate of the transmit data is lower than that of the control data, and the gain factors of the transmit data and control data are made β (<1) and 1,

respectively, on the transmit side. However, the symbol
rate of the transmit data is higher or lower than that
of the control data depending upon whether the transmit
data is voice data or image data, etc. In other words,
there are instances where the gain factor of the
transmit data is β and cases where the gain factor of
the control data is β. In such case, the second
embodiment determines which gain factor, i.e., the gain
factor of the control data or the gain factor of the
transmit data, is β and which is 1, changes the level
according and then executes decoding processing.

Fig. 3 is a block diagram illustrating a CDMA
receiver according to the second embodiment. Components
in Fig. 3 identical with those of the first embodiment
are designated by like reference characters. The second
embodiment differs from the first embodiment in the
following respects:

(1) a size comparator 41 is provided for
determining whether the power ratio (β^2 = Pd/Pc) is
larger or smaller than 1;

(2) a signal-level changing unit 42 is provided for
multiplying the level of the soft-decision transmit data
sequence output from the delay add-on unit 29 by $1/\beta$ if
the power ratio is smaller than 1 and Pd<Pc holds, and
for multiplying the level of the soft-decision transmit
data sequence output from the delay add-on unit 29 by 1
if the power ratio is larger than 1 and Pd>Pc holds;
and

(3) a signal-level changing unit 44 is provided for multiplying the level of the soft-decision transmit data sequence output from the delay add-on unit 28 by β if the power ratio is larger than 1 and Pd>Pc holds, and

5 for multiplying the level of the soft-decision transmit data sequence output from the delay add-on unit 28 by 1 if the power ratio is smaller than 1 and Pd<Pc holds.

In accordance with the second embodiment, even though power is reduced on the transmit side by

10 multiplying the level of the control data or transmit data by β, the level of the signal that has been reduced in power is multiplied by 1/β on the receive side, whereby the original level of the signal is restored. This is followed by the decoding of the signal. As a

15 result, decoding can be performed correctly even though the transmission powers of the control data and transmit data differ.

(D) Third embodiment

In spread-spectrum communications, e.g., spread-

20 spectrum communications based upon W-CDMA, interference between channels caused by non-linearity between spreading codes is a major factor that limits system capacity. In particular, since heavy interference from high-speed channels such as for transmitting moving

25 images puts pressure on the capacity of low-speed channels, how to suppress such interference is a major challenge insofar as assuring the capacity of low-speed channels is concerned. An interference canceller is a

device which suppresses interference by generating a replica of an interference signal using the results of demodulation of each receive channel and subtracting the replica from the receive signal.

5   Fig. 4 is block diagram illustrating one channel's worth of a CDMA receiver having an interference canceller. Specifically, the receiver includes an interference canceller 101, fingers 102_1 to 102_n, a RAKE combiner 103 and a decoder 104. The interference

10   canceller 101 includes interference cancellation units (ICU) 111_n ~ 111_n, which are provided for respective ones of receive channels, for generating and outputting interference replicas of the chip rates of the channels based upon the receive signals; a combiner 112 for

15   combining the interference replica signals of the respective channels; a filter 113 for limiting the band of the combined interference replica signals; a delay unit 114 for delaying the receive signal for a length of time required for generation of an interference replica;

20   and a subtractor 115 for executing interference suppression by subtracting the combined interference replica from the receive signal, thereby producing a residual signal.

The interference cancellation units 111_n ~ 111_n of

25   the respective channels generate interference replicas and produce replicates (replicates of control data and replicates of transmit data) of the transmit signal having the symbol rate. These replicates are referred

to as symbol replicas. The interference cancellation

units 111_n ~ 111_n are connected in parallel and shorten

processing time by processing all channels

simultaneously.

5   Each of the fingers 102_1 ~ 102_n has a despreader 121

for executing despread processing in sync with path

timing, which enters from a searcher (not shown),

thereby outputting a despread signal of the residual

signal that has undergone interference cancellation; a

10   combiner 122 for adding the symbol replica to the

despread signal; a channel estimating circuit 123 for

estimating a channel characteristic; and a channel

compensation unit 124 for eliminating phasing by

applying channel compensation processing to the output

15   signal of the combiner 122 using the channel estimation

signal. The RAKE combiner 103 combines the channel-

compensated signals output from the fingers, generates

soft-decision data and inputs the soft-decision data to

the decoder 104.

20   Fig. 5 is a block diagram illustrating a symbol

replica generator in an interference cancellation unit

for generating replica signals of control data and

transmit data from a receive signal. The symbol replica

generator is particularly applicable to a case where

25   control data and transmit data has been transmitted at

different powers. The symbol replica generator has a

structure similar to that of the CDMA receiver of the

second embodiment and components thereof identical with

those of this CDMA receiver are designated by like reference characters.

The symbol replica generator differs from the CDMA receiver of the second embodiment in the following

5   respects:

(1) a decision unit 44 is provided at the output of the signal-level changing unit 42 for rendering a hard decision based upon the signal level and outputting a hard-decision transmit data sequence;

10   (2) a decision unit 45 is provided at the output of the signal-level changing unit 43 for rendering a hard decision based upon the signal level and outputting a hard-decision transmit data sequence;

(3) means (a conversion table) 46 is provided for

15   changing replica reliability RC1 of the transmit data and replica reliability RC2 of the control data based upon the power ratio;

(4) a symbol replica signal generator 47 is provided for generating a replica of transmit data on

20   the transmit side by multiplying the hard-decision transmit data sequence output from the decision unit 44 by the replica reliability RC1 conforming to the power ratio; and

(5) a symbol replica signal generator 48 is

25   provided for generating a replica of control data on the transmit side by multiplying the hard-decision transmit data sequence output from the decision unit 45 by the replica reliability RC2 conforming to the power ratio.

Fig. 6 illustrates an example of the conversion
table 46. The table stores a weighting coefficient
(reliability RC1) for the data channel and a weighting
coefficient (reliability RC2) for the control channel in

5   association with each power ratio [= (power Pd of the
transmit-data signal)/(power Pc of the control-data
signal)]. Because reliability increases with an
increase in signal power, a larger weighting coefficient
is used. In a case where the power ratio (= Pd/Pc) is

10 less than 1, the signal power of the control channel is
larger than that of the transmit data. Accordingly, the
weighting coefficient RC2 of the control channel is
increased and the weighting coefficient RC1 of the data
channel is decreased. Conversely, if the power ratio (=

15 Pd/Pc) is greater than 1, the signal power of the
control channel is less than that of the transmit data.
Accordingly, the weighting coefficient RC2 of the
control channel is decreased and the weighting
coefficient RC1 of the data channel is increased.

20   Thus, in accordance with the third embodiment,
replica reliability is changed based upon the power
ratio. In other words, the higher the reception power,
the greater the replica reliability is made. This makes
it possible to improve the reliability of the symbol

25 replica generated.

(E)   Fourth embodiment

Fig. 7 is a block diagram illustrating an
interference replica generator in an interference

cancellation unit for generating an interference replica from a receive signal. The interference replica generator is particularly applicable to a case where control data and transmit data has been transmitted at

5   different powers. Components in Fig. 7 identical with those of the third embodiment of Fig. 5 are designated by like reference characters. The interference replica generator of the fourth embodiment differs from the replica generator of the third embodiment in the

10 following respects:

(1) a re-spreading multiplexer 51 is provided for spreading replicas of the control data and transmit data using respective ones of transmit-side spreading codes, and mapping the replicas as I- and Q-channel components

15 of an I-Q complex plane to thereby perform multiplexing and replicate the transmit signal;

(2) means (a second conversion table) 52 is provided for changing replica reliability RC of the transmit signal based upon the power ratio; and

20 (3) an interference replica generator 53 is provided for generating a replica of the transmit signal by multiplying the replicated transmit signal by the replica reliability RC that conforms to the power ratio.

Fig. 8 illustrates an example of the second

25 conversion table 52. The table stores a weighting coefficient (reliability RC) for the transmit signal in association with each power ratio [= (power Pd of the transmit-data signal)/(power Pc of the control-data

signal)]. The replica reliability RC is reduced if the

power ratio is small and is increases if the power ratio

is large. The reason for this will now be described.

Since the symbol rate is fixed at 15 kbps on the

5 control channel, the spreading factor is fixed for this

channel. However, since the symbol rate on the data

channel varies, so does the spreading factor. If the

symbol rate is high and the spreading factor is low,

gain (process gain) due to spreading will be low. As a

10 consequence, it is necessary for the quality of the data

channel to be maintained on at the same level as that of

control channel. Gain factor is used to control this.

If the spreading factor of the data channel is low,

the power at the end of the transmit antenna must be

15 increased. This is for the purpose of maintaining the

same quality even though the spreading factor varies.

In particular, a low spreading factor on the data

channel means that the symbol rate is high and that data

such as image data is being transmitted rather than

20 voice. In general, data such as image data requires a

higher communication quality than voice data. If the

spreading factor of the data channel is low, therefore,

the power at the transmit antenna is raised. Thus, when

the spreading factor of the data channel is low (power

25 ratio = Pd/Pc > 1), transmission power, i.e., reception

power, is higher than when the spreading factor of the

data channel is high (power ratio = Pd/Pc < 1). In the

second conversion table 52, therefore, the larger the

power ratio (= Pd/Pc), the larger the reliability RC is made; the smaller the power ratio (= Pd/Pc), the smaller the reliability RC is made.

Thus, in accordance with the fourth embodiment,
5 replica reliability is changed based upon the power ratio. More specifically, the higher the reception power, the higher the replica reliability is made. This makes it possible to raise the reliability of a generated replica.

10 Thus, in accordance with the present invention, the power ratio is not deduced based upon rate information contained in control data as in the prior art. Rather, the power ratio is calculated upon obtaining the power of the transmit-data signal and the power of the
15 control-data signal. This makes it possible to shorten the processing time needed for calculating the power ratio. Further, the fact that processing time is shortened means that it is possible to reduce the scale of circuitry needed to add on a processing delay.

20 Further, in accordance with the present invention, the level of whichever signal has been reduced in power by having its signal level multiplied by β on the transmit side is multiplied by 1/β on the receive side, whereby the original level of the signal is restored.
25 This is followed by the decoding of the signal. As a result, decoding can be performed correctly even though the transmission powers of the control data and transmit data differ.

Further, in accordance with the present invention, the level of the transmit-data signal is raised if the power ratio (= Pd/Pc) of transmit-data signal power Pd to control-data signal power Pc is less than 1 and the level of the control-data signal is raised if the power ratio is greater than 1. As a result, even though the signal level of the transmit-data signal or of the control-data signal is lowered on the transmit side, whichever signal level has been lowered can be restored automatically and decoding processing can be executed correctly on the receive side.

Further, in accordance with the present invention, replica reliability is changed based upon the power ratio. More specifically, the higher the reception power, the higher the replica reliability is made. This makes it possible to raise the reliability of a generated symbol replica and the reliability of an interference replica.

As many apparently widely different embodiments of the present invention can be made without departing from the spirit and scope thereof, it is to be understood that the invention is not limited to the specific embodiments thereof except as defined in the appended claims.